Power conversion architecture for grid interface at high switching frequency

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Abstract—This paper presents a new power conversion architecture for single-phase grid interface. The proposed architecture is suitable for realizing miniaturized ac-dc converters operating at high frequencies (HF, above 3 MHz) and high power factor, without the need for electrolytic capacitors. It comprises of a line-frequency rectifier, a stack of capacitors, a set of regulating converters, and a power combining converter (or set of power combining converters). The regulating converters have inputs connected to capacitors on the capacitor stack, and provide regulated outputs while also achieving high power factor, with twice-line-frequency energy buffered on the capacitor stack. The power combining converter combines power from the individual regulated outputs to a single output, and may also provide isolation. While this architecture can be utilized with a variety of circuit topologies, it is especially suited for systems operating at HF (above 3 MHz), and we introduce circuit implementations that enable efficient operation in this range. The proposed architecture is demonstrated for an LED driver operating from 120 V enable efficient operation in this range. The proposed approach HF (above 3 MHz), and we introduce circuit implementations that circuit topologies, it is especially suited for systems operating at isolation. While this architecture can be utilized with a variety of circuit topologies, it is especially suited for systems operating at HF (above 3 MHz), and we introduce circuit implementations that enable efficient operation in this range. The proposed architecture is demonstrated for an LED driver operating from 120 V enable efficient operation in this range. The proposed approach HF (above 3 MHz), and we introduce circuit implementations that is suitable for realizing miniaturized ac-dc converters operating at high frequencies (HF, above 3 MHz) and high power factor, without the need for electrolytic capacitors. It comprises of a line-frequency rectifier, a stack of capacitors across the ac line voltage, and thus the buck PFC should be designed with high voltage active devices. This high voltage requirement for grid interface also results in large parasitic capacitance, low achievable switching frequencies, and large passive components, and consequently in low power density.

Here we propose a new grid-interface power conversion architecture that addresses these problems. It can achieve reasonably high power factor (e.g., about 0.9, which is sufficient for many applications such as LED driver circuits), while dynamically buffering twice-line frequency energy using small capacitors operating at moderate voltages and voltage swings.

The proposed converter thus shares the benefits of some “third port” architectures for buffering line frequency energy (e.g., [6]–[12]), in that it can achieve high energy storage density without the need for electrolytic capacitors. Moreover, it enables high switching frequencies to be achieved (above 3 MHz) with relatively low voltage components, yielding high efficiency and high power density. Section II of the paper describes the structure and operation of the proposed grid interface architecture, and illustrates its characteristics with simulations. Section III of the paper presents a circuit implementation that leverages the advantages of the proposed architecture to operate efficiently at 5–10 MHz, and presents experimental results demonstrating the proposed system. Finally, Section IV concludes the paper.

II. SYSTEM ARCHITECTURE AND CHARACTERISTICS

The proposed architecture is illustrated in Fig. 1. It comprises a line-frequency rectifier, a stack of capacitors across the rectifier output, a set of regulating converters having inputs connected to capacitors on the capacitor stack and outputs that are regulated to a desired level, and a power-combining converter (or set of power combining converters) that combines the power from the outputs of the regulating converters to provide a single output.

The line-frequency rectifier draws current from the grid during a portion of the cycle, with a waveform controlled by the operation of the regulating converters. The capacitor stack provides most or all of the twice-line-frequency energy buffering, such that the converter can provide high power factor without buffering energy at the system output. One or
The proposed grid interface power conversion architecture comprises a line-frequency rectifier, a stack of capacitors, a set of regulating converters, and a power combining converter.

The power-combining converter has a plurality of inputs connected to the regulating converter outputs, wherein the power-combining converter draws energy from the regulating converter outputs and delivers the combined power to the converter system output. The power-combining converter may provide one or more of: voltage balancing among the regulating converter outputs, isolation, voltage transformation, a portion of twice-line-frequency energy buffering, and additional regulation of the output. The power-combining converter may be designed as a multi-input converter, or as a set of single-input converters which take inputs connected to ones of the regulating converter outputs and supply a single output. Because the power combining converter operates from a low, narrow-range input voltage, and needn’t (in many designs) provide regulation, it can be designed to be very compact. One possibility in this case is to design it for operation at HF or VHF [15]. Another possibility (when isolation is not required) is to design it using switched-capacitor techniques, as demonstrated here.

A. Line-Frequency Energy Buffering

Before introducing an example implementation with a specific regulating and power combining circuit topology, we show how the stacked converter structure (i.e., stack of capacitors and regulating converters) can be used to buffer twice-line-frequency energy and provide high power factor.

Fig. 2 shows a simplified model of the front end of the proposed grid interface architecture along with example operating waveforms. The two current sources \((i_1\) and \(i_2\)) model the currents drawn by the regulating converters. The circuit cycles in two phases across a half line cycle. During phase 1, the input ac voltage amplitude is lower than the total voltage of the stacked capacitors; the full-bridge rectifier is off and there is no current drawn from the grid. During this phase, capacitors \(C_1\) and \(C_2\) are discharged by the regulating converters and the voltage across the capacitor stack decreases. When the input ac voltage amplitude reaches the total capacitor stack voltage, the full-bridge turns on and the circuit enters phase 2.

During phase 2, the total voltage of stack capacitors tracks the rectified ac input voltage, and the input current follows the sum of the currents into \(C_1\) and regulating converter 1 (as well as tracking the sum of the currents into \(C_2\) and regulating converter 2). When the regulating converters no longer discharge the capacitor stack voltage fast enough to
• phase 1 – full-bridge is off and conducts zero input current

\[ i_{ac}(t) = 0 \]  

\[ P_o(t) = v_{c1}(t) i_1(t) + v_{c2}(t) i_2(t) \]  

• phase 2 – full-bridge is on and conducts \( i_{ac}(t) \) input current

\[ v_{ac}(t) = V \sin \omega t = v_{c1}(t) + v_{c2}(t) \]  

\[ i_{ac}(t) = i_{c1}(t) + i_1(t) = i_{c2}(t) + i_2(t) \]  

\[ P_o(t) = v_{c1}(t) i_1(t) + v_{c2}(t) i_2(t) \]  

\[ i_1(t) = \frac{C_1}{C_2} \frac{v_{c2}(t)}{v_{c2}(t) - v_{c1}(t)} \left\{ \left( \frac{1}{C_1} + \frac{1}{C_2} \right) i_{in}(t) - \omega V \cos \omega t - \frac{P_o(t)}{C_2} \right\} \]  

\[ i_2(t) = \frac{1}{v_{c2}(t)} \left( P_o(t) - v_{c1}(t) i_1(t) \right) \]

follow the decrease in line voltage, the full-bridge turns off and the circuit enters phase 1.

Assuming that the regulating converters draw currents (averaged over a switching cycle of the regulating converters) \( i_1(t) \) and \( i_2(t) \), and that the power combining converter combines power (from the two regulating converters) without loss and continuously supplies the required output power \( P_o(t) \), the mathematical expressions for each phase are as shown in equations (1)–(11).

It should be noted that during phase 2, equations (10) and (11) are calculated from equations (5)–(8), and the \( i_1(t) \) and \( i_2(t) \) currents result in the pre-defined input current of the system over the line cycle providing good power factor. There are many relations among the stack capacitor values, power level, capacitor voltage variation, regulating converter operating range, and power factor. Thus, selecting appropriate topologies, design values and operating waveforms is essential.

A key design consideration is selection of the capacitor values \( C_1 \) and \( C_2 \). The capacitors are typically sized asymmetrically (one large, one small), such that one can both buffer the twice-line-frequency energy with reasonable voltage swing and provide a desired line-current pattern for high power factor.

Another key consideration in controlling the converter is to follow the desired input current waveform (and capacitor stack voltage pattern) over a line cycle. These patterns may be pre-computed as a function of desired output power \( P_o \) and/or output voltage, and applied to both maintain the desired output and input waveforms across operating condition. Waveform selection is accomplished by iteratively selecting waveform shapes and numerically calculating performance over a half line cycle using (1)–(11), with the requirement that the system both operate in periodic steady state over this interval and remain within the operating constraints of the regulating converters.

B. Circuit Simulation

To demonstrate the operation of the proposed architecture and illustrate how it achieves high power factor and buffers ac energy, we present time-domain simulations of the system front-end using the model of Fig. 2.

We illustrate how the currents of each regulating converter are calculated and how the capacitor stack voltage varies for a particular set of design parameters. We consider an ac-dc converter operating from 60 Hz, 120 \( V_{ac} \), and supplying 30 W of output power; this example matches the experimental system described in the following section. The stack capacitors are picked as \( C_1 = 1 \mu F \) and \( C_2 = 50 \mu F \). In addition, each regulating converter is assumed to be able to operate across a 35–100 V input voltage range and to be able to deliver power unidirectionally from its input to the power combining circuit (with the power combining converter assumed to combine powers from the regulating converters without loss).

For the proposed design and operating point, the initial voltages on capacitors \( C_1 \) and \( C_2 \) (at the line zero crossing) are 35 V and 70 V, respectively. Figs. 3–8 show the simulation results for this case. Fig. 3 shows the input current waveform programmed to be drawn from the ac line for this design at the specified 30 W output operating condition. From numerous iterative simulations, a folded-clipped-sinusoidal input current waveform is selected as a good operating waveform providing high power factor (about 0.9) and satisfying the system design constraints (That is, the input current waveform is selected as zero for part of the cycle, as a sinusoidal signal for part of the cycle, and as a constant minus the sinusoidal signal during part of the waveform.)

With the specified input current waveform and design parameters, the average currents of each regulating converter and stack capacitor voltages are calculated from equations (1)–(11) and plotted as shown in Figs. 4 and 5. As can be seen in Fig. 4, the current drawn by each regulating converter is always positive. Moreover, as shown in Fig. 5, the voltages of the two “stack” capacitors vary over the line cycle as...
they are dynamically charged and discharged by the regulating converters, remaining within the specified operating range. The input voltage of the regulating converters varies over 35–100 V (operating range of the regulating converter), and the system operates in periodic steady state over the line cycle (i.e., the capacitor voltages are the same at the beginning and end of the half line cycle.)

Fig. 6 shows the line voltage and total capacitor stack voltage over a half line cycle. When the full bridge rectifier conducts, the capacitor stack voltage tracks the line voltage. Once the line voltage falls below the total capacitor stack voltage, the rectifier ceases to conduct, as illustrated in Fig. 2 and described in section II-A. From Figs. 5 and 6 it can be seen that the asymmetric sizing of the stack capacitors enables the stack voltage to track the line voltage (and draw line current) over a large portion of the line cycle, while also buffering the twice-line-frequency energy.

The input power $P_{in}$ is drawn from the line and the output power (total of the powers drawn from the capacitor stack by the regulating converters) are shown in Fig. 7. The proposed architecture controls the regulating converters to buffer the twice-line-frequency energy on the stack capacitors such that the total output power from the two regulating converters is almost constant. As illustrated in Fig. 8, the two regulating converters split the total power over the line cycle, and each regulating converter is rated for the total (line-cycle-average) output power of the system.
As illustrated in the above example, the front-end of the proposed architecture accomplishes three functions: First, it draws power from the line at high power factor. Second, it buffers twice-line-frequency energy from the line on the capacitor stack, such that constant power can be delivered to the system output. Lastly, while it is not explicitly shown above, the front end steps down the large input voltage, and provides narrow-range regulated outputs for the power combining stage.

C. Design Tradeoffs

There are several trade-offs among the design parameters to be considered in realizing a design. The first is the relation between capacitor stack size and the operating voltage of regulating converters. Usually as one uses smaller stack capacitors (C1 and C2), the capacitor voltages vary across wider voltage ranges over the line cycle to buffer the twice-line-frequency energy. The regulating converters then needs to be operated over this wider voltage range, which can degrade the size and performance of the regulating converters. Another design consideration is between power factor and the operating voltage range of the regulating converters. As the regulating converter are operated across wider voltage ranges, the proposed ac-dc architecture can conduct current for a longer conduction time over the line cycle, providing higher power factor. However, again, the burden on the regulating converters increases. Lastly, bi-directional converter capability could improve the achievable power factor of the system and required buffer capacitance size, but makes the design of the regulating converters much more challenging.

It should be noted that in some cases (or for some power levels), high power factor and twice-line-frequency energy buffering cannot be met simultaneously with a given set of capacitor values. In such cases, the power combining converter may then needs to buffer some portion of twice-line-frequency energy to supply constant power to the load. Overall, the trade-offs are mainly restricted by the topology of the regulating converter.

D. System Characteristics

The proposed grid interface architecture we adopt has several advantages. One apparent benefit is the decreased voltage stress to the components in the regulating converters and the power combining converter relative to the line voltage. In comparison to common grid interface converter which must be rated for the grid voltage, each regulating converter of the proposed architecture instead operates up to about half of the grid voltage because of the stacked capacitor structure (with an increased number of “stack” capacitors and regulating converters, this voltage stress may be further reduced as illustrated in Fig. 9.) Moreover, the power combining converter, tied to the regulated outputs of the regulating converters, operates at both low voltage and narrow input voltage range. Large step down conversions are also more readily achieved, aided by the stacked nature of the front end conversion system and - in some cases - supplemented by further step down from the power combining converter.

It should be noted that with certain power combining topologies (e.g. the SC charge balance circuit as shown in Fig. 10 and described hereinafter), one of the two regulating converters can directly supply the system output, and the combining converter only need process a portion of the power. This can be regarded as reducing the redundant processing power in the converter, and contributes to improved efficiency [16].

Converters operating at high voltages and low currents operate at high impedance levels, and consequently utilize relatively large inductors and small capacitors (e.g., characteristic impedance \( Z_0 = \sqrt{L/C} \) scales as \( V/I \)). Furthermore, inductor and capacitor values scale down with increasing resonant frequency (e.g., \( f = 1/\sqrt{LC} \)). Thus, for a given topology, increasing frequency beyond a certain point may lead to capacitance values that are too small to be practically achievable (e.g., given parasitics), placing a practical bound on frequency and miniaturization. For miniaturization of converters at high voltage and low power, it is preferable to select system architectures and circuit topologies that require relatively low characteristic impedance values (i.e., small inductances and large capacitances) to reduce constraints on scaling up in frequency. The proposed architecture roughly divides the input voltage range of each regulating converter by two, by stacking two regulating converters, and thus decreases the required inductance and increases the allowable capacitance. Higher switching frequencies (bounded by practically achievable capacitance levels) are thus enabled by this approach. This consideration is further associated with converter topology selection, as described in Section III.

The difference between instantaneous input power from the line and output power (twice-line-frequency energy) should be buffered inside of the converter so that it needn’t be buffered at the system output. This twice-line-frequency energy \( (E_b = P_o / \omega_{line}) \) is not related to the switching frequency of the converter, but to the power level and the ac line frequency. By utilizing a relatively large voltage swing on the storage capacitors \( C_1 \) and/or \( C_2 \), small-valued capacitors can be employed (i.e., \( C(V+\Delta V)^2 - \frac{1}{2} CV^2 = \text{buffered energy} \)).
The proposed architecture enables film or ceramic capacitors to be employed instead of electrolytic capacitors, which can benefit lifetime, temperature rating, and reliability of the system.

The proposed architecture can be extended with many variations and many options of converter topologies. For example, as shown in Fig. 9, the architecture may provide an interface to universal ac grid voltage with an increased number of capacitors and subsystem blocks. Moreover, the number of capacitors and regulating converters that are used at a given time may be allowed to vary dynamically (e.g., depending upon whether the circuit is connected to 120 or 240 Vrms.) This enables greater flexibility of operation, and narrower component operating ranges than could otherwise be achieved.

III. IMPLEMENTATION AND EXPERIMENTAL RESULTS

A. Topology Selection

The proposed architecture enables substantial miniaturization through adoption of greatly increased switching frequencies for the regulating converters. To attain greater miniaturization, increases in switching frequency are necessary because the values of inductors and capacitors vary inversely with switching frequency. However, the sizes of passive components do not necessarily decrease monotonically with frequency, owing to magnetic-core loss, voltage breakdown, and heat transfer limits. In addition to loss considerations, the practical values of required components can also limit switching frequency (i.e., yielding impractical values compared to inherent parasitics as frequency is increased). This is a particular challenge in converter operating at high voltage and low current. Consequently, achieving substantial miniaturization through high frequency operation further relies upon appropriate passives design and careful selection of circuit topology to minimize the demands placed upon the passive components, especially the magnetic components.

To address the considerations and achieve high efficiency and high power density, the regulating converters are designed as inverted resonant buck converter and the power combining converter is designed as a switched capacitor circuit as shown in Fig. 10. The regulating converter is designed with single switch, diode, and small inductor, and operates at HF (3–30 MHz) similar to the regulation-stage design illustrated in [13], [14]. It is an “inverted” circuit in the sense that it is designed with “common positives.” Besides control methods, for much of its operating range, the topology acts like a quasi-square-wave ZVS buck converter with a low ratio of switching to resonant frequency [17]. Each regulating converter takes as an input one of the capacitor voltages (from the stack of capacitors) and provides a regulated voltage across its output capacitor. This regulating converter design has several benefits. First, it operates with ZVS or near-ZVS soft switching across the 35–100 V wide input voltage range. The single common-referenced switch (referenced to a slowly-moving potential) makes it suitable for operation at HF (3–30 MHz). Second, it requires only a single, small-valued inductor. Furthermore, it has very fast response (near single cycle) to input voltage transients and changes in the output current command. Finally, for a given input voltage, the output current is roughly proportional to transistor on-time, allowing a variety of control schemes to be employed.

TABLE I

<table>
<thead>
<tr>
<th>Stack of Capacitors</th>
<th>Regulating Converter</th>
<th>Power Combining Converter</th>
<th>Control</th>
</tr>
</thead>
<tbody>
<tr>
<td></td>
<td></td>
<td></td>
<td>Microcontroller Atmel ATtiny 1634</td>
</tr>
<tr>
<td></td>
<td>$C_1$ 1 $\mu F$ X7R Ceramic 100 V</td>
<td>$Q_{R1}, Q_{R2}$ GaN switch EPC 2012</td>
<td>Microcontroller Atmel ATtiny 1634</td>
</tr>
<tr>
<td></td>
<td>$C_2$ 225 $\mu F$ X7S Ceramic 100 V</td>
<td>D Schottky diode STPS30120DJF</td>
<td></td>
</tr>
<tr>
<td></td>
<td></td>
<td>L 800 nH 10 turns on a Micrometal P68-106</td>
<td></td>
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<tr>
<td></td>
<td></td>
<td></td>
<td>Microcontroller Atmel ATtiny 1634</td>
</tr>
<tr>
<td></td>
<td>$C_{f1}, C_{f2}$ 20 $\mu F$ X7R Ceramic 100 V</td>
<td>switch GaN switch EPC 2012</td>
<td></td>
</tr>
</tbody>
</table>

For much of its operating range, the topology acts like a quasi-square-wave ZVS buck converter with a low ratio of switching to resonant frequency [17]. Each regulating converter takes as an input one of the capacitor voltages (from the stack of capacitors) and provides a regulated voltage across its output capacitor. This regulating converter design has several benefits. First, it operates with ZVS or near-ZVS soft switching across the 35–100 V wide input voltage range. The single common-referenced switch (referenced to a slowly-moving potential) makes it suitable for operation at HF (3–30 MHz). Second, it requires only a single, small-valued inductor. Furthermore, it has very fast response (near single cycle) to input voltage transients and changes in the output current command. Finally, for a given input voltage, the output current is roughly proportional to transistor on-time, allowing a variety of control schemes to be employed.

We selected an interleaved switched-capacitor (SC) circuit for the power combining converter. This is an effective choice for high efficiency and power density, as the converter needn’t provide regulation [18]. The SC circuit draws energy from the two regulating converter outputs and supplies the single system output (which is also the output of one of the regulating converters). Because the switched capacitor circuit transfers charge without voltage regulation, and is designed with switches and capacitors, it can be operated high efficiency at low frequency with small converter size. In the proposed SC circuit, the capacitors $C_{f1}$ and $C_{f2}$ transfer charge from capacitor $C_{R1}$ to capacitor $C_{R2}$ and supply the combined power to the load. Since in this prototype the load is connected across the output of one of the regulating converter, the SC circuit only processes a portion of overall system energy. Moreover, if $C_{f1}$ and $C_{f2}$ are selected as much larger than $C_{R1}$ and $C_{R2}$, partial “soft charging” of the energy transfer capacitors can be achieved [19].

B. Implementation

To test the proposed architecture, we implemented an example system based on the topology described above. The system
is designed to supply 30 W to a 35 V dc output from a 120
\(V_{\text{rms}}\) AC 60 Hz input. We utilize the control strategy described
and demonstrated in simulation in Section II. The system
comprises a line-frequency bridge rectifier and a small filter
choke; a stack of two capacitors; a pair of regulating resonant-
transition buck converters; and an unregulated SC
power-combining converter having two inputs and an output
supplying the system output.

As shown in section II, the proposed architecture can buffer
the ac energy with \(C_1 = 1 \mu F\) \(C_2 = 50 \mu F\) at 30 W power
level. In selecting practical capacitors, it must be recognized
that the capacitance of high-k ceramic capacitors degrades
with bias voltage. Consequently, we used 1 \(\mu F\), 100 V X7R
capacitance for \(C_1\) and a (nominal) 225 \(\mu F\), 100 V X7S
ceramic capacitance for \(C_2\) in this prototype.

Table 1 shows the component selection of the inverted
resonant-transition buck converters used in the prototype. With
these values the regulating converters operate in the range of
5–10 MHz under soft-switching conditions over their input
voltage and power range. The SC circuit is designed with 20
\(\mu F\), 100 V X7R energy transfer capacitors and GaN switches
as presented in Table I, and operates at a fixed switching
frequency of 30 kHz.

As illustrated in section II, the proposed ac-dc architecture
dynamically buffers twice-line-frequency energy and draws a
pre-defined ac current with high power factor by modulating
two regulating converters over the line cycle. We used a
microcontroller to control the average current of each regu-
lating converter and synchronize operation over the line cycle
(Atmel, ATtiny 1634); Fig. 11 describes the control scheme.
The microcontroller detects the zero-voltage crossing of the
ac line voltage and resets the time state. The microcontroller
monitors the capacitor stack voltage (the input voltage of each
regulating converter) and sends updated pre-defined switch-
turn-on duration information to each regulating converter every
~80 \(\mu s\). In addition, the microcontroller generates the 30 kHz
50 % duty ratio switching signal (with dead time) for the SC
circuit.

C. Experimental Results

The prototype converter is designed to support up to 30 W
output at 35 V from 120 V\(_{ac}\). The prototype circuit of Fig. 10
was implemented on a 1.9 in x 1.4 in printed board as shown
in Fig. 12.

Fig. 13 shows measured voltage waveforms of the converter
at startup and during operation over the ac line cycle, when
powered from a Agilent 6812B ac power supply. Ch 2 (blue) is
the voltage across the capacitor \(C_2\), ch3 (purple, y: 50 V/div) is the total stack
capacitor voltage after the full-bridge, ch4 (green, y: 50 V/div) is the 120
\(V_{rms}\) ac line voltage, and ch M (red, y: 50 V/div) shows the voltage across
the capacitor \(C_1\). The capacitors \(C_1\) and \(C_2\) satisfy periodic-steady-state
operation over the line cycle, and dynamically buffer twice-line-frequency
energy.

Fig. 14 shows the measured input ac voltage and current.
The prototype converter showed 93.3% efficiency with 0.89
power factor for a 35 V dc 30 W load.

The volume of the prototype converter is measured, and the
“box power density” was calculated to 25 W/in\(^3\). It is
notable that this is much higher than the ~5 W/in\(^3\) found
for typical commercial LED drivers at this power rating,
even though we didn’t optimize component layout for box-
volume power density. The displacement volume was 0.23 in\(^3\)
yielding a “displacement power density” of 130 W/in\(^3\); this
illustrates the high power density achieved, and that layout
can readily provide a greatly improved “box power density”.

![Fig. 11. Block diagram showing the converter and control system. The microcontroller detects the zero crossing event of ac line voltage and resets the time state. The microcontroller monitors the capacitor stack voltage (the input voltage of each regulating converter) via a voltage divider and ADC, and sends updated switch-turn-on duration information to each regulating converter every ~80 \(\mu s\). The turn-on durations used over the line cycle are predetermined for the desired output power and input voltage and stored in a lookup table. In addition, the microcontroller generates the 30 kHz 50 % duty ratio switching signals (with dead time) for the SC circuit.](image1)

![Fig. 12. The prototype converter, implemented in a 1.9 in x 1.4 in printed board. This figure shows the front side and the back side of the PCB.](image2)

![Fig. 13. The implemented converter is connected to 120 \(V_{rms}\) ac line voltage with at 35 V output at 30 W power. The ac line voltage is realized with a Agilent 6812B ac power supply, and the figure shows the measured voltage waveform across the ac line cycle (x: 4 ms/div). Ch2 (blue, y: 50 V/div) is the voltage across the capacitor \(C_2\), ch3 (purple, y: 50 V/div) is the total stack capacitor voltage after the full-bridge, ch4 (green, y: 50 V/div) is the 120 \(V_{rms}\) ac line voltage, and ch M (red, y: 50 V/div) shows the voltage across the capacitor \(C_1\). The capacitors \(C_1\) and \(C_2\) satisfy periodic-steady-state operation over the line cycle, and dynamically buffer twice-line-frequency energy.](image3)
The proposed stacked-combined architecture can significantly decrease the voltage stress of the active and passive devices, enabling high-frequency operation and small size. Moreover good power factor is achieved while dynamically buffering twice-line-frequency ac energy with relatively small capacitors. The prototype implementation, which is suitable for LED driver applications, achieves 93.3% efficiency and 0.89 power factor while maintaining high frequency operation and small size (130 W/in³ displacement power density). The proposed architecture can be designed with different regulating and combining converter topologies, and can likewise be applied to the requirements of a variety of applications and power levels.

IV. CONCLUSION

A new ac-dc architecture suitable for single-phase grid interface at high switching frequency (above 3 MHz) is introduced and experimentally demonstrated. This new grid interface architecture is specifically intended for high frequency operation to deal with the needs of high efficiency, high power density, and high power factor for ac-dc applications. The proposed stacked-combined architecture can significantly decrease the voltage stress of the active and passive devices, enabling high-frequency operation and small size. Moreover good power factor is achieved while dynamically buffering twice-line-frequency ac energy with relatively small capacitors. The prototype implementation, which is suitable for LED driver applications, achieves 93.3% efficiency and 0.89 power factor while maintaining high frequency operation and small size (130 W/in³ displacement power density). The proposed architecture can be designed with different regulating and combining converter topologies, and can likewise be applied to the requirements of a variety of applications and power levels.

REFERENCES